

TITLE OF THE INVENTION

MATCHED FILTER AND RECEIVER FOR MOBILE RADIO

COMMUNICATION SYSTEM

5 FIELD OF THE INVENTION

This invention relates to a matched filter used in a path search in the receiver of a mobile radio communication system that utilizes a spread-spectrum signal. More particularly, the invention relates to a 10 matched filter capable of reducing power consumption and mounting area. The present invention relates further to a receiver which uses a matched filter.

BACKGROUND OF THE INVENTION

15 Mobile radio communication systems typified by cellular telephone systems have come into wide use rapidly in recent years. This increase in number of subscribers has been accompanied by a shift from analog to digital communication systems and a further transition to 20 next-generation systems is about to take place. One system that is currently the focus of attention, as such a next-generation communication system, is CDMA (Code Division Multiple Access), which is a communication system that relies upon spread-spectrum modulation.

25 According to the CDMA system, a user-specific spreading code sequence is assigned on a per-user basis. The transmitter transmits a transmission signal (modulated signal) the spectrum of which is spread by multiplying

transmission data by the spreading code sequence, and the receiver multiplies the received signal by a code sequence synchronized with symbol timing and identical with the spreading code sequence that was used on the transmit side,
5 thereby demodulating the received signal and recovering the transmitted data.

With this system, instead of assigning a different transmission frequency band or transmission time to each user in the manner of FDMA (Frequency Division Multiple Access) or TDMA (Time Division Multiple Access), a common transmission band and transmission time are assigned to all users so that the signals of respective users are transmitted at the same time in the same frequency band that has been allocated to the system. It is known that
10 the CDMA system makes it possible to increase system capacity (number of subscribers) in comparison with other multiple-access systems such as FDMA and TDMA by skillfully controlling and suppressing interference that occurs among
15 multiple users sharing the same frequency band and
20 transmission time.

In a mobile radio communication system, a so-called multi-path phenomenon occurs. This is a phenomenon in which a signal that has been transmitted from a transmitter arrives at a receiver through a plurality of different paths
25 upon being reflected by buildings and other structures. In such instances the receiver receives a multi-path signal resulting from a combination of multiple signals whose propagation delays differ depending upon the paths

traveled.

The CDMA system makes it possible to achieve path diversity by taking advantage of such a multi-path signal. A specific example known in the art is the RAKE receiver.

5 The path diversity effect also contributes to an increase in CDMA system capacity.

Fig. 10 is a block diagram illustrating an example of the configuration of a conventional RAKE receiver. As shown in Fig. 10, a CDMA radio signal is received by an
10 antenna 101 and a receive circuit 102 and then is multiplied with a local carrier in a frequency mixer 103, whereby the signal is converted to a baseband signal. The output of the frequency mixer 103 is sampled at a predetermined rate by a sampling circuit (not shown) and converted by an A/D converter (not shown) and is then supplied to a matched
15 filter 104 as a stream of digital values.

The matched filter 104 executes despreading process using a spreading code supplied by a spreading code generating circuit, which is not shown. The output of the
20 matched filter 104 is supplied to a path-timing detector 105 and RAKE combiner 106. The path-timing detector 105 and matched filter 104 constitute a path searcher which determines the effective paths to be added in the RAKE combiner 106.

25 The RAKE combiner 106 accepts the receive signal from the matched filter 104 at the timing supplied by the path-timing detector 105, adds the signals of the prescribed number of effective paths (fingers) coherently

by aligning the phases of these path signals and then outputs the result. The output signal is evaluated by a symbol detection circuit (not shown) and the demodulated data is obtained. If necessary, the amplitudes of the path
5 signals are weighted at the phase alignment.

The matched filter 104 can be configured by a transversal-type matched filter in which the number of taps is equal to the number of chips of one symbol period, i.e., to the spreading factor, wherein the chip values of a
10 spreading code are supplied as the tap values. In a case where over-sampling is performed by the sampling circuit, the number of taps is the product of the spreading factor and the number of over-samplings. Each tap is supplied with a code sequence in which each chip of the spreading
15 code is repeated in accordance with the number of over-samplings, or with a code sequence in which numerical values of 0 have been interpolated among each chip value of the spreading code in accordance with the number of over-samplings.

20 Fig. 11 is a diagram illustrating an example of a configuration of the matched filter 104, which has M-number of taps (where M is a natural number). This example illustrates a matched filter of the well-known transversal type.

25 As shown in Fig. 11, the matched filter comprises M-number of delay elements (D) 201, 202, . . . , 20(M-1), 20M; M-number of multipliers 211, 212, 213, . . . , 21(M-1),

21M; and (M-1)-number of adders 221, 222, 223, . . . , 22(M-1).

The multipliers are supplied with respective ones of tap values C1, C2, C3, . . . , C(M-1), CM, multiply the outputs of the respective delay elements by the respective 5 tap values and outputs the products. The outputs of the multipliers are added by the adders and the total of the outputs of all multipliers is obtained from the adder 221 as the final output of the matched filter.

The delay elements 201 - 20M each represent a delay 10 of one sampling interval. In a case where spreading factor T of transmitted signal and sampling rate of the input signal to the transversal-type filter are equal, the number of taps M is equal to T. If the input signal undergoes 2 times over-sampling, $M = 2T$ holds.

15 The tap values C1 - CM are supplied with the chip values of the spreading code. More specifically, if the spreading codes are "+1, +1, -1, +1, -1, +1, +1, . . .", then the tap values "+1, +1, -1, +1, -1, +1, +1, . . ." are supplied in order starting from C1. If the input signal 20 undergoes 2 times over-sampling, then tap values "+1, +1, +1, +1, -1, -1, +1, -1, +1, +1, +1, +1, . . ." or tap values "+1, 0, +1, 0, -1, 0, +1, 0, -1, 0, +1, 0, +1, 0, . . ." are supplied in order starting from C1.

Thus, the matched filter multiplies input data of 25 M samples and a spreading code of M chips, together chip by chip, and obtains the total of the products as the output, and this output indicates the degree of correlation between the input signal and the spreading code. Accordingly, if

a multi-path signal is supplied as the input signal to the matched filter, the sum of products is calculated chip by chip while staggering timing, successively, over one period of the spread code and the output result is monitored, 5 then the reception timing of a signal having strong correlation, i.e., the reception timing of each path signal contained in the multi-path signal, can be determined.

For example, in the receiver shown in Fig. 10, the path-timing detector 105 compares the output result of the 10 matched filter 104 with a predetermined threshold value and, when the threshold value is exceeded, the path-timing detector 105 notifies the RAKE combiner 106, thereby giving notification of the timing of the path signals that are to be combined.

15 In a case where the path-timing detector 105 and RAKE combiner 106 have a receive buffer corresponding to one period of the spreading code, the path-timing detector 105 can retain the output result from the matched filter 104 over one period of the spreading code, thereby making it 20 possible to detect a prescribed number of timings at which large results are obtained and report these timings to the RAKE combiner 106.

This processing of the matched filter can be implemented using a general-purpose microprocessor or a 25 digital signal processor (DSP).

As mentioned above, the matched filter requires a number of taps equal to the spreading factor or to the product of the spreading factor and the number of

over-samplings. Therefore, if the spreading factor is 512, at least 512 taps will be required.

Since a 512-tap matched filter requires 512 delay elements, 512 multipliers and 511 two-input adders, the 5 scale of the circuitry is extremely large. In reality, because over-sampling is usually carried out in order to achieve reception with good precision, the number of taps becomes actually many times larger, as a consequence the problem of scale is compounded.

10 In addition, since all of these very large numbers of operational elements operate simultaneously in synchronized with the sampling clock, power consumption increases in dependence upon the number of the taps.

Further, in a case where the function of the matched 15 filter is implemented by a processor, a high-speed processor is required because it is necessary to execute the product-summing processing within one sampling clock interval a number of times equivalent to the number of taps per symbol period. For example, if this arithmetic 20 processing is executed using a processor that controls the overall receiver, the load on the processor will become so large that other processing may be affected. If a separate dedicated processor is used, this will enlarge the mounting area of the receiver and an increase in power 25 consumption will be unavoidable.

If the matched filter that is necessary for a receiver requires a large mounting area and/or power consumption, this will be a further impediment to achieving a

size/power-consumption reduction in a mobile radio communication terminal. This may also lead to less call standby-time and talk-time.

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SUMMARY OF THE INVENTION

Accordingly, an object of the present invention is to provide a matched filter that does not require a high-speed processor and that consumes less power.

The gist of the present invention is a matched filter
10 having a plurality of multiplication means for multiplying an input-sample stream and a predetermined code sequence together in predetermined unit by predetermined unit; wherein the results of multiplication by the plurality of multiplication means are summed and output, characterized
15 in that the input-sample stream is a stream obtained by sampling a multi-path signal; and in that the matched filter has control means for determining which multiplication means actually perform multiplication among the plurality of multiplication means; a minimum number of
20 multiplication means necessary for a period of time during which there arrive path signals regarded as being effective among a plurality of path signals contained in the multi-path signal.

The gist of present invention in another aspect
25 thereof is a matched filter for obtaining and outputting correlation between an input-sample stream and a code sequence having predetermined periodicity, characterized in that the input-sample stream is a stream obtained by

sampling a multi-path signal, and in that the matched filter has multiplication means of a number equivalent to a number of codes constituting at least one period of the code sequence; addition means for summing outputs of the 5 multiplication means and outputting the sum as a value representing correlation of the input-sample stream to the code sequence; and control means for determining which multiplication means actually perform multiplication among the multiplication means, a minimum number of 10 multiplication means necessary for a period of time during which there arrive path signals regarded as being effective in the multi-path signal, and controlling said determined multiplication means to multiply said code sequence of one symbol length and each value of said input-sample stream.

15 The gist of present invention in another aspect thereof is a matched filter characterized by having: a plurality of delay elements connected in series and having an externally supplied input-sample stream input to one end thereof; a plurality of multiplication means to which 20 outputs from the plurality of delay elements are applied as a first input signal and externally supplied data is applied as a second input signal for multiplying the first and the second input signals together; addition means for summing outputs of the plurality of multiplication means 25 and outputting the sum as a value representing correlation of the first input signal to the second input signal; and control means for dividing the plurality of delay elements and multiplication means into blocks, performing

enable/disable control block by block, and supplying each of the plurality of multiplication means contained in a block that has been enabled with a code constituting a partial code sequence of a predetermined code sequence; 5 and in that the input-sample stream is a stream obtained by sampling a multi-path signal, and from among the blocks of the multiplication means, the minimum number of blocks of multiplication means necessary for a period of time during which there arrive path signals regarded as being 10 effective in the multi-path signal are enabled by enable/disable control as a block which actually performs multiplication.

The gist of present invention in another aspect thereof is a receiver for a mobile radio communication 15 system that uses a matched filter according to the present invention.

The gist of present invention in another aspect thereof is an arithmetic unit characterized by functioning as a matched filter according to the present invention.

20

BRIEF DESCRIPTION OF THE DRAWINGS

The accompanying drawings, which are incorporated in and constitute a part of the specification, illustrate embodiments of the invention and, together with the 25 description, serve to explain the principles of the invention.

Fig. 1 is a block diagram showing an example of the principle components of a CDMA receiver to which a matched

filter according to the present invention can be applied;

Fig. 2 is a block diagram illustrating an example of a configuration of a demodulator 504 and RAKE combiner 505 in the matched filter in Fig. 1;

5 Fig. 3 is a diagram useful in describing a method of deciding maximum amount of delay;

Fig. 4 is a circuit diagram showing an example of the configuration of a matched filter according to an embodiment of the present invention;

10 Fig. 5 is a block diagram showing an example of a configuration of a variable-delay shift register in an integrating circuit;

Fig. 6 is a circuit diagram showing a configuration of the matched filter of Fig. 4 in a case where $N=4$, $n=1$
15 hold;

Fig. 7 is a diagram useful in describing the content of operations performed in a matched filter of conventional configuration, wherein one sequence of spreading code is composed of 16 bits and the number of taps is 16;

20 Figs. 8A and 8B are diagrams useful in describing the content of operations performed by a partial filter 301 of the matched filter according to the embodiment of the present invention under conditions equivalent to those of Fig. 7;

25 Fig. 9 is a diagram useful in describing operation of a shift register in an integrating circuit;

Fig. 10 is a block diagram showing an example of the overall configuration of a RAKE receiver according to the

prior art; and

Fig. 11 is a circuit diagram showing an example of the configuration of a transversal filter used as a matched filter according to the prior art.

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DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

(Configuration of receiver)

A preferred embodiment of the present invention will now be described in detail with reference to the drawings.

10 Fig. 1 is a block diagram showing an example of the principle components of a receiver of a CDMA communication system to which a matched filter according to the present invention can be applied. The implementation shown in Fig. 1 shows components related to signal processing up to a point prior to symbol detection following conversion to a baseband signal via a frequency mixer and then conversion to a stream of digital values while sampling is performed at a predetermined rate. The stream of digital values is represented simply as an input signal.

20 A cell searcher 501 in Fig. 1 decides the cell to which the communication terminal having this receiver should synchronize. In CDMA systems, a received signal having the strongest reception strength (or best quality) is used for synchronization among multiple signals
25 received from a plurality of base stations at the same time. In order to accomplish this, which base station to synchronize to (and which spreading code sequence to use) is decided by the cell searcher 501.

The cell searcher 501 further performs synchronization acquisition and synchronization tracking and supplies a matched filter 502 and a despreader/demodulator 504 (sometimes simply referred to 5 as "demodulator" hereinafter) with symbol timing and a multi-path delay T_d in one symbol period.

The matched filter 502 receives the symbol timing from the cell searcher 501 and, using the input signal and spreading code, sends an output indicative of degree of 10 correlation to a path timing detector 503. The latter detects effective-path timings of a prescribed number from the output of the matched filter 502 and outputs the path 15 timings to the demodulator 504. The demodulator 504, which has demodulation circuits of the effective-path number (the number of path signals to be combined) predetermined in a manner described later, despreads the effective-path signals based upon the symbol timing received from the cell 20 searcher 501 and the path timings received from the path timing detector 503.

A RAKE combiner 505 weights the effective paths 25 output by the demodulator 504, combines these path signals by aligning phases and outputs the result to a symbol detection circuit, which is not shown. The operation for aligning the phases can be implemented by using, as a reference, the phase of each path in the pilot signal contained in the received signal.

Fig. 2 is a block diagram illustrating an example of a configuration of the despreader/demodulator 504 and

RAKE combiner 505 shown in Fig. 1. Fig. 2 illustrates implementation for a case where the number of effective paths is three. Numerals 54, 55 and 56 denote multipliers for phase alignment and weighting.

5 The demodulator 504 has demodulation circuits 51, 52 and 53, the number of demodulators being equal to the number of effective paths. The demodulation circuits 51, 52, 53 have respective spreading code generators 511, 521, 531 which, on the basis of the effective-path timing 10 information detected by the path-timing detector 105 and the symbol timing from the cell searcher 501, generate spreading code sequences at timings that differ from one another and supply these code sequences to corresponding correlators 512, 522, 532, respectively, whereby 15 processing of despreading the effective-path signals is executed. It should be noted that the path timing information is supplied separately to the individual spreading code generators.

The outputs of the correlators 512, 522 and 532 are 20 supplied to an input terminal of respective multipliers 54, 55 and 56 of the RAKE combiner 505. Supplied to the other input terminals of the multipliers 54, 55 and 56 are coefficients α, β and γ , respectively, for performing weighting and for aligning phases by canceling out phase 25 fluctuation of the paths measured in advance.

These coefficients are prepared by periodically receiving a specific signal, such as a pilot signal on a control channel, the content of which is known in advance,

and detecting phase-fluctuation of each effective paths by using a phase-fluctuation detection circuit (not shown).

The effective-path signals whose phases have been
5 aligned and which have been weighted by the multipliers
54, 55 and 56 in the RAKE combiner 505 are combined by an
adder 57, with the resulting signal being output to a symbol
detection circuit (not shown).

Next, reference will be had to Fig. 3 to describe
10 symbol timing and method of deciding multi-path delay in
the cell searcher 501.

The cell searcher 501 has a well-known symbol timing
detection circuit (not shown) using a serial search
acquisition circuit or matched filter. In any case, by
15 despreading the input signal using the spreading code
generated within the cell searcher, the correlation
between the spreading code and the input signal is
determined over one period of the spreading code sequence
and symbol timing is decided using the timing for which
20 the strongest correlation is obtained.

Fig. 3 represents schematically the correlation,
which is obtained in the cell searcher 501, between a
spreading code sequence and the input signal. In the
example of Fig. 3, the largest correlation peak is
25 determined as the start time of the symbol period, and the
time difference between the start time and the time at which
the final peak exceeds a predetermined threshold value (as
shown in Fig.3) is decided upon as the maximum amount of

delay of the multi-path signal.

In this embodiment, the cell searcher 501 decides that an effective-path signal is a signal having a peak that exceeds the predetermined threshold value. The 5 threshold value is determined in advance based upon reliability information such as the signal-to-noise ratio and signal-to-interference ratio of the multi-path signal.

(Principle)

The operating principle of the matched filter 10 according to the present invention will now be described. In a conventional matched filter, within one symbol period, the product-summing calculation is performed a number of times equivalent to the square of the number of chips (number of taps) that form at least one symbol period (one 15 sequence) of a spreading code sequence, and a path search is conducted for paths having a delay corresponding to up to one symbol period. Accordingly, if the spreading code has a period of 16 bits and there is no over-sampling, the product-summing calculation should be performed 16×16 20 = 256 times in a 16 sampling periods.

In an ordinary mobile radio communication system, however, if the communication distance between a transmitting station and a receiving station is comparatively short, the maximum amount of delay of the 25 multi-path signal is short in comparison with one symbol period and there are instances where effective paths do not diverge over the entire symbol period. Further, in a case where the particular purpose is a path search, if the

timing of the final arriving effective path can be detected, it will not be necessary to perform an operation to search for paths that have no possibility of arriving after being delayed beyond this timing.

5 Reducing the amount of computation increases available processing time for individual operations such as product-summing during one symbol period and therefore decreases the requirement of high-speed processing. In addition, with the computation reduction, a calculation
10 that has to be performed within a sampling period provided by one delay element can be executed using a plurality of sampling periods. This makes it possible to reduce, further, the number of taps actually used. For example, if the spreading factor is 16, the over-sampling rate is
15 one and the maximum amount of delay is eight sampling periods, then a search for paths having amounts of delay of 9 - 16 sampling periods (in the above example) becomes unnecessary. The amount of calculation, therefore, is halved. As a result, computation that needs to be
20 performed 16 times in one sampling period now need be performed only eight times. As a consequence, the processing speed of the matched filter that performs the operation can be halved or the number of taps used in the path search can be halved from 16 to 8.

25 Further, employing a matched filter in which the number of taps used can be adjusted and the adjustment of the number of taps used in dependence upon the maximum delay that is detected periodically makes it possible to deal

with a maximum delay that fluctuates.

(Configuration of matched filter)

Fig. 4 is a block diagram showing the configuration of a matched filter according to an embodiment of the present invention. The matched filter in Fig. 4 has a plurality (N, which is a natural number equal to 2 or greater) of partial filters 301, 302, . . . , 30N; a gate 311, for delivering a selected outputs of the partial filters 301 - 30N designated by a control signal from a controller 341; 10 an adder 321 for adding all outputs from the gate 311; an integration circuit 331 for integrating the output of the adder 321; and the controller 341, which controls the overall matched filter.

Each partial filter is a matched filter having a predetermined number (m, which is a natural number equal to 2 or greater) of taps. Serially connecting N-number of the partial filters 301 - 30N construct a matched filter having $m \times N$ taps overall. Partial filters 301 - 30N are supplied by the controller 341 with values (spreading code) 20 applied to each of the taps and with an enable/disable control signal for starting/stopping operation on a per-partial-filter basis.

The integration circuit 331, which is constituted by, e.g., an adder 332 and an $n \times m$ (where n is the number 25 of active partial filters)-stage variable-delay shift register 333, described later, retains ($m \times n$)-number of results of addition obtained by summing the output of the adder 321 every $m \times n$ outputs.

An example of the configuration of the variable-delay shift register 333 is illustrated in Fig. 5. Specifically, the shift register is constituted by $m \times N$ serially connected delay elements (D) and a gate 334. From 5 signals (the maximum number of which is N) input to it every m -number of serially connected delay elements, the gate 334 selects one and outputs it to the adder 332 based upon a gate control signal supplied from the controller 341. This arrangement makes it possible to vary the amount of 10 signal delay by the control signal. The content of the variable-delay shift register 333 is reset (to zero) by a reset signal from the controller 341.

The controller 341 is supplied by the cell searcher 501 with the symbol timing and maximum delay time, as 15 described earlier.

(Operation)

Let T_s represent the sampling period of the input signal and let n (where n is a natural number and $N \geq n \geq 1$ holds) represent the number of partial filters that have 20 been enabled by the enable/disable control signal of controller 341. Since the n -number of partial filters construct a matched filter having $n \times m$ taps, it is possible to process an input signal having a period of time equal to $n \times m \times T_s$.

25 Accordingly, if we let T_d represent the maximum delay time of the multi-path signal, n is determined from the following expression:

$$n \times m \times Ts \geq Td > (n-1) \times m \times Ts \quad (1)$$

In general, Td is smaller than $n \times m \times Ts$. In a case where use is made of n -number of partial filters, therefore, $(N-n)$ -number of partial filters corresponding to the 5 remaining $(N-n) \times m$ taps are disabled and have their operation inhibited by the enable/disable control signal. This makes it possible to reduce power consumption by a wide margin.

Let C_1, C_2, \dots, C_N represent N subsequences of the 10 spreading code obtained by dividing the (one sequence f) spreading code into N subsets, then each subsequence can be denoted as follows.

$$C_1 = (c_{1,1}, c_{1,2}, \dots, c_{1,m})$$

$$C_2 = (c_{2,1}, c_{2,2}, \dots, c_{2,m})$$

15 .

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$$C_N = (c_{N,1}, c_{N,2}, \dots, c_{N,m})$$

In the description rendered below, the j -th value in an i -th subsequence is represented by $c_{i,j}$ ($N \geq i \geq 1, m \geq j \geq 1$).

20 The controller 341 first finds the n that satisfies the above-cited Expression (1) from the maximum delay time Td supplied by the cell searcher 501, the already known sampling period Ts and the number m of taps of each partial filter. The controller then enables the n -number of 25 partial filters 301 - 30n, disables (inhibits the operation of) the other partial filters 30(n+1) - 30N and outputs a control signal to the gate 311 so that only the outputs

of the partial filters 301 - 30n are delivered to the adder 321.

Next, at the taps (multipliers) of the enabled partial filters 301 - 30n, the controller 341 sets the 5 corresponding subsequences C1 (c1,1 - c1,m) - Cn (cn,1 - cn,m) of the spreading code.

As described with reference to Fig. 11, the partial filters 301 - 30n multiply the input signal by the spreading code supplied to each tap and output the sums of the products.

10 The outputs of the partial filters 301 - 30n are supplied to the adder 321 through the gate 311, and the adder 321 outputs, to the integration circuit 331 every sampling period Ts, the sum total of the operational results from the partial filters 301 - 30n.

15 In the integration circuit 331 the adder 332 adds the output of the variable-delay shift register 333 and the operational result from the adder 321 and stores the sum in the variable-delay shift register 333.

Upon elapse of time $n \times m \times Ts$, the controller 341 20 sets the subsequences C (n+1) - C (2n) at the taps of the partial filters 301 - 30n. New subsequences are subsequently set successively every $n \times m \times Ts$ and then the above-described process is repeated. After that, if the symbol timing is entered from the cell searcher 501, 25 the initial subsequences C1 - Cn will be set again. In response to input of the symbol timing, all values that have been stored in the variable-delay shift register 333 are output to the path-timing detector 105 and the content

of the register is reset to prepare for despreading of the next symbol.

As described with reference to Fig. 3, the path-timing detector 503 compares the output of the variable-delay shift register 333 with a threshold value and determines the timings of effective paths. If the stored content of the variable-delay shift register 333 can be read out at all times, the path-timing detector 503 compares the content of the variable-delay shift register 333 and the threshold value in parallel with the operation performed by the matched filter, whereby detection of effective paths will also be completed when the variable-delay shift register 333 is reset.

The operation of the matched filter according to this embodiment will now be described in greater detail with reference to Figs. 6 to 9. The following will be taken as an example in the description rendered below:

$m = 4$ as number of taps of each of partial filters 301 - 304;
20 16 bits for one sequence of spreading code;
 $N = 4$ as number by which the sequence is divided;
4Ts as maximum amount of delay; and
over-sampling rate is one (and hence one symbol period = 16Ts).
25 The controller 341 first finds the n that satisfies Expression (1) from the maximum delay time T_d supplied by the cell searcher 501 and the number m of taps of each partial filter. As a result, $n = 1$ is found. Since only

the partial filter 301 is effective in this case, the controller 341 turns on only a switch corresponding to the effective partial filter 301 among switches in gate 311 that correspond to the partial filters 301 - 304. The 5 controller turns off the other switches. Further, the controller enables the partial filter 301 and disables (halts operation of) the other partial filters 302 - 304 (see Fig. 6).

In this case, the matched filter according to this 10 embodiment is capable of reducing the amount of calculation per symbol period to $4/16 = 1/4$ in comparison with the matched filter of the conventional implementation. That is, with the matched filter of the conventional implementation, computation is performed over the entire 15 symbol period using all 16 taps simultaneously. Consequently, if we let $C (c_1, c_2, \dots, c_{16})$ represent one sequence of spreading code and let $d_1, d_2, \dots, d_{16}, d_{17}, \dots$ represent the sample data of the input signal, then, as shown in Fig. 7, the product-summing operation 20 is performed 16 times in each symbol period of 16Ts, and 256 product-summing operations are required in total.

However, the fact that the maximum amount of delay is 4Ts means that it will suffice if the search for paths having the delays 1Ts - 4Ts is conducted within one symbol 25 period. The operations involving Ts5 - Ts16 in Fig. 7 (the operations for searching for paths having delays 5Ts - 16Ts) are performed needlessly (assuming that these operations are for the purpose of path search).

In the matched filter of the conventional implementation, the product-summing operation ($Ts_1 - Ts_4$ in Fig. 7) performed in the search for paths having amounts of delay up to $4Ts$ is carried out $16 \times 4 = 64$ times. It will suffice if this operation is performed in 16 sampling periods ($16Ts$) corresponding to one symbol period. Accordingly, the same result can be obtained by performing the operation four times in one sampling period, i.e., by using only the four-tap partial filter 301.

In order to perform the operations indicated by $Ts_1 - Ts_4$ in Fig. 7 using the single partial filter 301, the subsequence of the spreading code supplied to the taps of the partial filter 301 is updated by the controller 341 every $4Ts$.

Figs. 8A and 8B illustrate the content of operations performed by the partial filter 301 over the period of time from the 1st sampling period Ts_1 to the 16th sampling period Ts_{16} .

Since the subsequences $C_1 - C_4$ are obtained by dividing one sequence $C(c_1, c_2, \dots, c_{16})$ by four, they satisfy the relations shown in Fig. 8A. In order to clarify the relationship with Fig. 7 showing the operation performed by the conventional implementation, the notation $c_1 - c_{16}$ will be used with regard to the sequences shown in Fig. 8B illustrating the operations performed by the partial filter 301.

First, since the subsequence $C_1 (c_1, c_2, c_3, c_4)$ is supplied to the taps in the sampling periods $Ts_1 - Ts_4$,

operations indicated in Fig. 7 by A, E, I, M, respectively, are performed.

When the operation in sampling period Ts4 ends, the controller 341 updates the subsequence supplied to the 5 partial filter 301 from C1 (c1, c2, c3, c4) to C2 (c5, c6, c7, c8). The partial filter 301 performs the operations in the sampling periods Ts5 - Ts8 using the subsequence C2. These operations correspond to operations B, F, J, and N in Fig. 7.

10 Similarly, operations are performed using the subsequence C3 (c9, c10, c11, c12) in the sampling periods Ts9 - Ts12 and the subsequence C4 (c13, c14, c15, c16) in the sampling periods Ts13 - Ts16, whereby the operations C, G, K, O, D, H, L and P shown in Fig. 7 are carried out.

15 In order to obtain the results of the operations that were performed heretofore in the sampling periods Ts1 - Ts4 from the operational results provided by the partial filter 301, operational results acquired every 4Ts should be integrated four times. Accordingly, the above- 20 mentioned integration is realized by setting the output tap of the variable-delay shift register 333 to the $(n \times m)$ -th stage, i.e., to the fourth stage.

Fig. 9 illustrates the change in the content of the variable-delay shift register 333 in the sampling periods 25 Ts1 - Ts16. In Fig. 9, Ts1 - Ts16 indicated at the stages of the variable-delay shift register 333 signify the results (see Fig. 8B) obtained in the sampling periods Ts1 - Ts16, respectively. As should be evident from Fig. 9,

the result of performing addition every 4Ts accumulates in each stage of the variable-delay shift register 333 in the 16th sampling period Ts16. These results are the operational results that were obtained heretofore in the 5 sampling periods Ts1 - Ts4 (see Fig. 7), and it will be understood that a path-search result similar to that of the prior art can be obtained by having the path-timing detector 105 use the content of the variable-delay shift register 333.

10 (Other embodiments)

In the foregoing embodiment, a case with the maximum amount of delay Td equals to m times Ts where m is the number of taps of the partial filter is described. However, it goes without saying that a matched filter can be constructed 15 in similar fashion even if Td is not a multiple of Ts. In such case needless computation over a period of time less than $m \times Ts$ will be performed a number of times. Even so, however, the power-consumption reducing effect of the present invention can be obtained satisfactorily.

20 Further, the greater the number N of divisions, the finer the number of taps can be controlled. However, this increases the number of switches in the gate and the number of signal lines for control signals. Moreover, enable/disable control owing to a fluctuation in the 25 maximum delay and processing for generating spreading-code subsequences supplied to the taps tend to occur more frequently, which will lead to the increase of control complexity. For this reason, the number of divisions

should be determined suitably in conformity with the amount of load on the controller.

Further, in a case where a receiver is constructed using the matched filter according to the present invention,
5 the maximum amount of delay detected by cell searcher is supplied to the matched filter with arbitrary time interval defined by relevant number of symbol periods.

In the embodiment set forth above, delays involved in processing such as detection of maximum amount of delay
10 by the cell searcher, path search by the path-timing detector 105 using the detected maximum amount of delay, and demodulation and phase alignment based upon the results of the path search, as well as delays in processing within the matched filter, have been ignored in the description
15 in order to facilitate an understanding of the embodiment. However, it goes without saying that the signals used in these processing operations can be adjusted, in time, by using buffers or the like.

In addition, in the embodiment set forth above, only
20 a case in which the matched filter is implemented using dedicated hardware is described. However, it goes without saying that the present invention is applicable even in a case where equivalent processing is implemented by software using a general-purpose processor such as an MPU
25 or DSP. In such case the performance required of the MPU or DSP will not be as high because of the reduction in amount of computation. This means that the MPU or DSP may be time-shared by other operation in addition to the matched

filter operation. Even in a case where a dedicated processor is used, it is possible to reduce the power consumption.

In accordance with the present invention, as described above, only a number of taps required solely for computation that is necessary are used in a matched filter employed in a path search for detecting effective paths from a multi-path received signal. In addition, a spreading code sequence is divided and supplied to the taps.

10 This makes it possible to realize a matched filter in which power consumption is suppressed by a wide margin in a form adapted to maximum delay time of the multi-path signal.

As many apparently widely different embodiments of the present invention can be made without departing from the spirit and scope thereof, it is to be understood that the invention is not limited to the specific embodiments thereof except as defined in the appended claims.